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## Contenido

DESARROLLO DE SOFTWARE SCADA PARA PLANTA PILOTO DE CONCRETO SECO CON PROTOCOLO ETHERNET/IP .....	10-27
Yolanda Pérez Pimentel, Ismael Osuna Galán	
SISTEMA AUTOMÁTICO DE INSPECCIÓN DE COMPONENTES MEDIANTE VISIÓN POR COMPUTADORA .....	28-44
Iván César Palacios Aguay, Ramiro Velázquez Guerrero	
MAXIMUM PRINCIPLE FOR TIME MINIMIZATION OF CIRCUIT DESIGN PROCESS .....	45-62
Alexander Zemliak	
SIMULACIÓN BASADA EN AGENTES PARA EL CONTROL INTELIGENTE DE SEMÁFOROS MEDIANTE LÓGICA DIFUSA .....	63-82
Héctor Rafael Orozco Aguirre, Saul Lazcano Salas, Víctor Manuel Landassuri Moreno	
ANALYSIS OF DIFFERENT STRATEGIES FOR CIRCUIT OPTIMIZATION .....	83-97
Alexander Zemliak, Fernando Reyes Cortés	
A NEURO-FUZZY BASED CONTROL OF A SIMULATED SOFC IN A GRID CONNECTED ENVIRONMENT .....	98-114
Sohail Khan, Juan Carlos Olivares Galvan, Rafael Escarela-Perez	
SINTONIZACIÓN DE UN CONTROLADOR PI APLICADO A UN HORNO EXPERIMENTAL A PARTIR DE LA IDENTIFICACIÓN DE MÚLTIPLES PUNTOS DE LA RESPUESTA EN FRECUENCIA UTILIZANDO UN ALGORITMO GENÉTICO .....	115-131
Cecilia de los A. Keb Chulín, César I. Coyoc y Coyoc, J. Rubén Lagunas Jiménez, Víctor M. Moo Yam	
DETECCIÓN ACTIVA DE FALTAS EN SISTEMAS DE EVENTOS DISCRETOS .....	132-152
Karen Hernández-Rueda, María E. Meda-Campaña, Bernardo Haro-Martínez	
METODOLOGÍA PARA LA IMPLEMENTACIÓN DEL MPM EN VHDL Y LA EMULACIÓN DE AMPLIFICADORES DE POTENCIA EN UNA TARJETA FPGA .....	153-173
Edgar Allende Chávez, José Ricardo Cárdenas Valdez, José Alejandro, Galaviz Aguilar, Andrés Calvillo Téllez, José Cruz Nuñez Pérez	
ANÁLISIS DE RENDIMIENTO DE LA PC ODROID C2 PARA SU USO EN ESQUEMAS DE CIUDADES INTELIGENTES .....	174-192
Ernesto Bardales Hernández, Saúl Lazcano Salas	
DESIGN AND FABRICATION OF A 64-QAM MODULATOR FOR ANALYSIS OF SIGNALS BETWEEN STAGES .....	8
Jorge Andrés Hernández Carrillo, José Ricardo Cárdenas Valdez, Virgilio Rosendo Pérez, Manuel de Jesús García Ortega, Andrés Calvillo Téllez	
ESTUDIO DE UNA ANTENA DE MICROCINTA FRACTAL TIPO E PARA LA BANDA DE LOS 2.4 GHZ .....	210-227
Iván R. González Rangell, Javier Vargas Sánchez, Genaro Hernández Valdez, Mario Reyes Ayala, J. R. Miranda Tello, Edgar A. Andrade González	
DISEÑO DE UN DEMODULADOR DE FM MEDIANTE PLL PARA LA INTERROGACIÓN DE SENSORES INTERFEROMÉTRICOS DE FIBRA ÓPTICA .....	228-248
Jesús Lorenzo Cisneros Hernández, Alejandro Rodríguez Antonio, Abimael Jiménez Pérez, José Mireles Jr. García, Rafael E. González Landaeta, Ángel Saucedo Carvail	
TRANSMISIÓN-RECEPCIÓN DE AUDIO VÍA LUZ VISIBLE .....	249-265
Sergio Sandoval Reyes, Arturo Hernández Balderas	
SENSOR CAPACITIVO DE ALERTA PARA IDENTIFICAR IMPUREZAS EN ACEITE DE MOTORES DIESEL .....	266-282
Hiram U. Luna López, Antonio Ramos Carrasco, María Elena Anaya Pérez, Dainet Berman Mendoza	
EFFECTO DE LA LONGITUD DEL DIÁMETRO EN LA ESTABILIDAD TÉRMICA DE LA CAPA LIBRE DE LAS MEMORIAS RAM MAGNÉTICAS .....	283-295
Marco A. Escobar, Rafael Guzmán-Cabrera, Miguel Torres-Cisneros, Jorge Ramón Parra-Michel, Rafael Martínez-Peláez	
DISEÑO DE SISTEMAS HIPERCAÓTICOS PARA IMPLEMENTACIÓN EN DISPOSITIVOS LÓGICOS PROGRAMABLES ENFOCADO A APLICACIONES DE SEGURIDAD .....	296-307
Jorge Gustavo Vázquez Duran, Ramón Ramírez Villalobos, Luis Néstor Coria de los Ríos, Manuel de Jesús García Ortega	
DISEÑO E IMPLEMENTACIÓN DE UN SISTEMA DE MEDICIÓN COMBINADA DE 4-PUNTAS .....	308-320
Francisco Javier Arizaga Ayala, Arturo III Espinoza Duarte, José Antonio Gallardo Cubedo, Armando Gregorio Rojas Hernández	
IMPLEMENTACIÓN DE BLOQUES PARA CONTROLADORES DIFUSOS ANALÓGICOS CON CIRCUITOS CMOS Y OPAMPS .....	321-334
Edgar López Delgado, Luis Alejandro Flores Oropeza, Luis Enrique Arámbula Miranda, Alfonso Vela Rivera, Martín Isaac Falcón Segovia	
PROTOTIPO DIDÁCTICO PARA NIÑOS DE PRIMARIA BASADO EN LA IDENTIFICACIÓN DE EMOCIONES Y SUS CONSECUENCIAS .....	335-351
Erick López Ornelas, Rocio Abascal Mena	
OBTENCIÓN DEL MÁXIMO ANCHO DE BANDA PARA LA ADQUISICIÓN Y RECONSTRUCCIÓN DE SEÑALES ANALÓGICAS CON LA TARJETA SPARTAN 3E .....	352-367
Enrique Gerardo Hernández Vega, Jorge Alberto Ortiz Gallo, Daniel Eduardo Morales Fernández, Alejandro Verdusco Hernández	
MÉTODOS NUMÉRICOS EN INGENIERÍA UAM AZCAPOTZALCO: BAOC (BIG ACADEMIC OPEN COURSE) .....	368-387

Hugo Pablo Leyva, Rafaela Blanca Silva López, Rafael Morales Gamboa	
CASO APLICATIVO DEL SISTEMA DE GESTIÓN DIGITAL: GESTIÓN DE ESPACIOS FÍSICOS .....	388-408
Rafaela Blanca Silva López, César Arostégui Ramírez, Iris Iddaly Méndez Gurrola, Hugo Pablo Leyva	
DETECCIÓN DE NECESIDADES Y DEFINICIÓN DE CONTENIDOS PARA LA ENSEÑANZA DE LA METODOLOGÍA DEL PERIODISMO DE DATOS: EL CASO DE DATAISTA .....	409-425
Belén Alazáquez Cortés,Zayra Monserrat Miranda Aguirre, Jocelyn Lizbeth Molina Barradas, Dra. Rocío Abascal Mena	
DIGITAPRENDE: UNA APLICACIÓN PARA LA ALFABETIZACIÓN DIGITAL DE ADULTOS MAYORES .....	426-444
Daniel Martínez Espino, Alba Rocío Núñez Reyes, Dra. Rocío Abascal Mena	
SISTEMA DE EVALUACIÓN POR COMPETENCIAS INTEGRADO A UNA PLATAFORMA EDUCATIVA INSTITUCIONAL .....	445-461
Victor Hugo Medina Sandoval, Arturo García Nevares, Miquel Àngel Rodríguez Ortiz	
DISEÑO Y CONSTRUCCIÓN DE PROTOTIPO DE ENTRENAMIENTO PARA PRÁCTICAS EN INSTRUMENTACIÓN Y CONTROL .....	462-478
Eladio Flores Martínez, Pablo Reyna Guerra, José Luis Jiménez Reyes, Javier Garrido Meléndez, Quetzalcoatl Cruz Hernández Escobedo	
SIMULACIÓN "HARDWARE IN THE LOOP" DE UN INVERSOR TRIFÁSICO CONECTADO A LA RED ELÉCTRICA479-498	
Manuel Tlapa Juárez, Edgar Peralta Sánchez, Juan Marcos Ruiz Dávila, Sergio Alejandro Cardaña Moreno, Félix Quirino Morales	
SISTEMA DE CÁLCULO DEL CONSUMO ELÉCTRICO DE LA UAM AZCAPOTZALCO .....	499-514
Rodrigo Vázquez López, Eduardo Campero Littlewood, Felipe González Montañez, Juan Carlos Olivares Galván, Raúl Arturo Ortiz Medina	
MODULO DE CONTROL DE CARGA PARA EVALUAR CELDAS DE COMBUSTIBLE -HARDWARE- .....	515-533
Shirley Yahaira Echánove Gómez, Marco Antonio Rodríguez Blanco, Juan Manuel Tadeo Sierra Grajeda, Luis Enrique Vidal Burelo	
MODELADO Y CONTROL DE UN CONVERTIDOR BOOST EN DCM EMPLEADO EN UN SISTEMA FOTOVOLTAICO PARA TRABAJAR EN MODO RED Y EN MODO ISLA .....	534-554
Miguel Angel Abundis Fong, Oscar Carranza Castillo, Jaime José Rodríguez Rivas, Rubén Ortega González	
MÉTODO DE INSTRUMENTACIÓN INDIRECTA BASADO EN ONDAS ACÚSTICAS DERIVADAS DE VIBRACIONES MECÁNICAS PARA LA ESTIMACIÓN DE VELOCIDAD ANGULAR EN MAQUINARIA ROTATIVA .....	555-574
Enrique Gerardo Hernández Vega, Sergio Iván Chavarría Estrada	
IMPLANTACIÓN DE UNA LPWAN PARA MONITOREO DE TEMPERATURA Y HUMEDAD EN UN INVERNADERO .....	575-595
José Ignacio Vega Luna, Mario Alberto Lagos Acosta, Gerardo Salgado Guzmán, Víctor Noé Tapia Vargas, Francisco Javier Sánchez Rangel, José Francisco Cosme Aceves	
DISEÑO DE UN CIRCUITO DE CONTROL DE ILUMINACIÓN PARA UN SISTEMA FORMADOR DE IMÁGENES DE PURKINJE .....	596-615
Armando Gómez Vieyra, Ezequiel Martínez Solís, Juan Jesús Ocampo Hidalgo, Karla Beatriz Vergara Vázquez, Uriel Calderón Uribe, Geovanni Hernández Gómez	
DISEÑO E INTEGRACIÓN DE UNA COMPUTADORA A BORDO PARA VUELOS ESTRATOSFERICOS .....	616-634
Lauro Santiago Cruz, Indira Citallí Cortés Sánchez, Mario Alberto Mendoza Bárcenas	
REDUCCIÓN DE CROSS-TALKING POR MEDIO DEL USO DE FOCALIZADORES EN APLICACIONES DE ULTRASONIDO .....	635-648
Jovan Alejandro Ramírez Guzmán, Ignacio Herrera Aguilar, Gerardo Águila Rodríguez, Oscar Osvaldo Sandoval González	
DESIGN, CONSTRUCTION AND CHARACTERIZATION OF A THREE-CHANNEL COSMIC RAY DETECTOR BASED ON ALUMINUM BLOCKS ELECTRONICS .....	649-668
Luis Arceo, Julián Félix	
DISEÑO, CONSTRUCCIÓN Y PRUEBAS DE UN DETECTOR HÍBRIDO DE RAYOS CÓSMICOS DE 4 CANALES .....	669-686
Francisco Javier Rosas Torres, Julián Félix	
INSTRUMENTACIÓN VIRTUAL DE UN SISTEMA DE GENERACIÓN EOLOELÉCTRICO INTERCONECTADO A LA RED .....	687-707
Adolfo Rafael López Núñez, Jesús Darío Mina Antonio, Roberto Carlos Gómez Hernández, Gabriel Calderón Zavala, Oscar Hernández Martínez	
SISTEMA DE ADQUISICIÓN DE DATOS DE BAJO COSTO PARA UN INVERNADERO BASADO EN TECNOLOGÍA DE ACCESO LIBRE .....	708-722
Felipe de Jesús Becerra Woo, Araceli Gárate García, Tania Aglaé Ramírez del Real, Ervin Jesús Alvarez Sánchez	
DISEÑO E IMPLEMENTACIÓN DE SENSORES DE GAS QCM DE ALTA SENSIBILIDAD PARA UNA NARIZ ELECTRÓNICA .....	723-740
Juan Jesús Jiménez Arellano, Severino Muñoz Aguirre, Juan Castillo Micoxatl, Georgina Beltrán Pérez, José Lorenzo Muñoz Mata	
INSTRUMENTACIÓN Y MONITOREO POR RED INALÁMBRICA DE SENSORES MEDIANTE XBEE PARA UN PROCESO DE POLIMERIZACIÓN .....	741-763
Cristian Mena Saucedo, Brian Manuel González Contreras, Miguel Ángel Munive Rojas, Fermin Martínez Solís	
DISEÑO E IMPLEMENTACIÓN DE UN MULTÍMETRO DIGITAL CON FUNCIONES AMPLIADAS DE BAJO COSTO764-784	
Rafael García Arredondo, Juan Carlos Gómez Cortez, Diego de Jesús Piedra Arvizu, José Eleazar Peralta López, Francisco Javier Pérez Pinal, Luis Antonio Ramírez Arredondo, Julio Cesar Regalado Sánchez	
DISPOSITIVO TELE MÉTRICO PARA MONITOREO DE FRECUENCIA CARDIACA Y SATURACIÓN DE OXÍGENO785-805	
Lorena Lomelí Herrera, Federico Aguayo Ríos, Rafael Martínez Peláez	

DETECCIÓN DE FALLA DE RODAMIENTO EN UNA CADENA CINEMÁTICA VÍA EMISIÓN ACÚSTICA .....	806-823
Luis Alejandro Romero Ramírez, Luis Morales Velázquez, Roque A. Osornio Ríos, René de Jesús Romero Troncoso, Daniel Morfíligo Sotelo	
SIMULADOR TRIDIMENSIONAL DE LA CINEMÁTICA DEL ROTOR DE UN AEROGENERADOR TRIPALA CON BASE EN LA CONVENCIÓN D-H .....	824-839
Ana Patricia Matus Vicente, Miguel Ángel Hernández López, Francisco Aguilar Acevedo, J. Jesús Arellano Pimentel	
METODOLOGÍA PARA LA INTEGRACIÓN DE UN MANIPULADOR MÓVIL BAJO SOFTWARE LIBRE .....	840-854
Oswaldo Alquirisirí Quecha, Francisco Aguilar Acevedo, Ignacio Algreto Badillo, J. Jesús Arellano Pimentel	
MÉTODO EXPERIMENTAL DE ESTIMACIÓN DE LA FUNCIÓN DE TRANSFERENCIA DE UN MOTOR DE CD UTILIZANDO ENCODER DE CUADRATURA .....	855-873
Jorge Fernando Vera Centeno, Ignacio Herrera Aguilar, Gerardo Águila Rodríguez, Oscar Osvaldo Sandoval González, Blanca Estela González Sánchez	
ROBOT CARTESIANO DE 3 GDZ PARA INSPECCION DE ESFUERZOS RESIDUALES MEDIANTE PRINCIPIO DE FOTOELASTICIDAD .....	874-892
Angel Vergara Betancourt, Fernando García Ortiz, Jose Guadalupe Gaona Reyes, Carlos Cortés Martínez	
DISEÑO Y SIMULACIÓN DE RODILLA MECÁNICA MONOCENTRICA .....	893-912
José Alexis Hernández Aguilar, Irvin Jesús Álvarez Sánchez, Andrés López Velázquez	
SISTEMA DE RECONOCIMIENTO DE VOCALES DE LA LENGUA DE SEÑAS MEXICANA .....	913-928
Eliuh Cuecucha Hernández, José Javier Martínez Orozco, Daniel Méndez Lozada, Adán Zambrano Saucedo, Aldrín Barreto Flores, Verónica Edith Bautista López, Salvador Eugenio Ayala Raggi	
BRAZO ROBOTICO CONTROLADO POR MEDIO DE VISION COMPUTACIONAL UTILIZANDO UN KINECT .....	929-948
Celina Villocaña González, María Teresa Orvañanos Guerrero, Eduardo Rodríguez Figueroa	
SIMULACIÓN DEL CONTROL Y LA COORDINACIÓN DE UN ROBOT EXPLORADOR EN UN AMBIENTE AGRÍCOLA .....	949-967
Marisol Rodríguez Cuevas, Andrés Fernando Jiménez López, Pedro F. Cárdenas H.	
APROXIMACIÓN AL RECONOCIMIENTO DE EMOCIONES FACIALES BASADO EN POSICIÓN DE PUNTOS DE INTERÉS .....	968-979
Victor Manuel Álvarez Pato, Ramiro Velázquez Guerrero	
IMPLEMENTACIÓN DE EFECTOS DE SONIDO PARA GUITARRA ELÉCTRICA EN LA TARJETA C6713 DSK .....	980-999
Claudia Gómez Borrás, Javier Alducin Castillo	
SEGMENTACIÓN DE IMÁGENES APLICANDO LA HERRAMIENTA COMPUTACIONAL P3S .....	1000-1017
Antonio Orantes Molina, Irwin Jovany Salinas Vargas, Raúl Cruz Barbosa, Rosebet Miranda Luna, Verónica Rodríguez López	
ANÁLISIS DEL MÉTODO DE CORRIMIENTO DE FASE PARA ESCANEÓ Y RECONSTRUCCIÓN 3D DE OBJETOS. 1018-1035	
Carlos Alberto Ramos Arrequin, Juan Carlos Moya Morales, Rodrigo Escobar Diaz Guerrero, Jesús Carlos Pedraza Ortega	
METODOLOGÍA PARA LA CORRECCIÓN DE DISTORSIÓN GEOMÉTRICA Y RECONSTRUCCIÓN 3D DE UN OBJETO MEDIANTE PERFILOMETRÍA WAVELET 1D .....	1036-1053
Claudia Victoria López Torres, Gonzalo Elias Blanco Silva, Jesús Carlos Pedraza Ortega, Juan Manuel Ramos Arrequin, José Emilio Vargas Soto, Mayra Azucena Cintora García	
COMPARACIÓN DE LAS TÉCNICAS DE DETECCIÓN DE CRUCE POR CERO Y LA TRANSFORMADA Z-CHIRP PARA MEDIR FRECUENCIAS EN EL RANGO ULTRASÓNICO .....	1054-1070
Guadalupe Aguilar Cerda, Luis Morales Velázquez	
PROPUESTA DE UN ENTRENADOR MIOELÉCTRICO BASADO EN UNA APLICACIÓN MÓVIL .....	1071-1090
Humberto de la Cruz Regalado, Carlos Edgar López Barrera, Eduardo Emmanuel Rodríguez López, Luis Mariano Sandoval González, Alfredo Ramírez García	
CONSTRUCCIÓN DE MAPAS DE ISÓCRONAS PARA LA ZONA PONIENTE DE LA CIUDAD DE MÉXICO .....	1091-1105
Erick López-Omelas, Rocío Abascal Mena, Santiago Avilés Vázquez	
ANÁLISIS DE UN SISTEMA DE ENFRIAMIENTO DEL CPU DE UNA COMPUTADORA EMBEBIDA POR MEDIO DE UNA CELDA PELTIER .....	1106-1120
Victor Daniel Tejeda Mejía, Miguel Angel Olivares Robles, Pedro Guevara López	
INTEGRACIÓN DE UN SISTEMA CEREBRO COMPUTADORA EMPLEANDO SOFTWARE LIBRE .....	1121-1139
Irving Ulises Hernández Miguel, Alejandro Jarillo Silva, Victor Alberto Gómez Pérez	
CASO APLICATIVO DEL SISTEMA DE GESTIÓN DIGITAL: GESTIÓN DE PROYECTOS DE INVESTIGACIÓN .....	1140-1158
Iris Idaly Méndez Gurrola, César Augusto Briseño Moreno, Rafaela Blanca Silva López	
REALIDAD AUMENTADA CON MARCADORES CUADRADOS Y NATURALES PARA NAVEGACIÓN QUIRÚRGICA .....	1159-1179
Eliana Margarita Aguilar Larrarte, Oscar Andrés Vivas Albán, José María Sabater Navarro	
DESARROLLO DE UN PROCESO DE AUTENTICACIÓN FACIAL EN UN SISTEMA ANDROID UTILIZANDO EL ALGORITMO LDA (ANÁLISIS DE DISCRIMINACIÓN LINEAL) .....	1180-1198
Francisco Emiliano Aguayo Serrano, Jesús Carlos Pedraza Ortega, Edgar Alejandro Rivas Araiza, José Erik Rivas Araiza .....	1199-1220
SIMULACIÓN DE ESTRATEGIAS DE BÚSQUEDA EN ANIMALES CON POSIBLES APLICACIONES EN COMPUTACIÓN Y ROBÓTICA .....	1199-1220
Joel Ricardo Jiménez Cruz	
SISTEMA PARA EL MONITOREO DE OPINIÓN CENTRADO EN ENTIDADES A PARTIR DE TWITTER .....	1214
José Alejandro Reyes Ortiz, Ezra Saucedo Vargas, Angeles Belém Priego Sánchez	
CLASIFICACIÓN DE REPORTES CLÍNICOS PARA APOYAR EL DIAGNÓSTICO DEL CÁNCER .....	1239-1256

José Alejandro Reyes Ortiz, Beatriz Adriana González Beltrán, Mireya Tovar Vidal ANÁLISIS DE ATAQUES DE RED DEL TIPO DHCP SPOOFING, TCP SYN FLOOD Y PAQUETES MALFORMADOS. 1257-1276	
Josué Cirilo Cruz, Arturo Zúñiga López, Carlos Avilés Cruz, Juan Villegas Cortez COMPARATIVA KINECT VS MYO APPLICANDO LA PRUEBA NASA-TLX EN UN ENTORNO DE RV1 PARA INSPECCIÓN EN AEROGENERADORES .....	1277-1297
Daniel Cantón Enriquez, J. Jesús Arellano Pimentel, Miguel Ángel Hernández López, Francisco Aguilar Acevedo INGENIERÍA ONTOLÓGICA APLICADA EN EL DISEÑO DE UN SISTEMA DE ONTOLOGÍAS PARA LA GESTIÓN DE HORARIOS .....	1298-1319
Maricela Claudia Bravo Contreras, Francisco Pavón Gutiérrez, José Alejandro Reyes Ortiz, Roberto Alfonso Alcántara Ramírez MODELOS DE TECNOLOGÍAS DEL BIG DATA ANALYTICS Y SU APLICACIÓN EN SALUD .....	1320-1339
Gustavo Verduzco Reyes, Ernesto Bautista Thompson, Jorge A. Ruiz Vanoye, Alejandro Fuentes Penna IMPLEMENTACIÓN EN "HARDWARE IN THE LOOP" DEL SISTEMA CARRO-PÉNDULO INVERTIDO CON BASE EN EL MICROCONTROLADOR HERCULES RM57L843 DE TEXAS INSTRUMENTS .....	1340-1359
Marcelino Martínez Aragón, Fermín Hugo Ramírez Leyva, José Anibal Arias Aguilar INVENTARIO DE MÁQUINAS EXPENDEDORAS USANDO UNA LPWAN .....	1360-1380
José Ignacio Vega Luna, Mario Alberto Lagos Acosta, Gerardo Salgado Guzmán, Víctor Noé Tapia Vargas, Francisco Javier Sánchez Rangel, José Francisco Cosme Aceves ANÁLISIS COMPARATIVO DE LOS TIEMPOS DE EJECUCIÓN SOBRE SBC PARA DOS SISTEMAS OPERATIVOS DE TIEMPO REAL .....	1381-1397
Diana Lizet Rodríguez Baldovinos, Jose Luis Cano Rosas, Pedro Guevara López SUPERVISIÓN DE TEMPERATURA Y HUMEDAD PARA EL CÁLCULO DE BALANCE ENERGÉTICO EN UN INVERNADERO CON TIEMPOS DE MUESTREO OBTENIDOS DE FORMA EXPERIMENTAL .....	1398-1413
Sergio Eduardo Luna Arauz, Andrés Alfonso Andrade Vallejo, Pedro Guevara López, Juan Enrique Rubiofz Panta COMPARACIÓN DE TARJETAS ARDUINO UNO ORIGINALES Y CLONES COMO INSTRUMENTO DE MEDICIÓN ... 1414-1428	
Miguel Angel Bañuelos Saucedo DISPOSITIVO DE ILUMINACIÓN LED CON INCORPORACIÓN DE ELECTRÓNICA DIGITAL Y CONTROL DESDE ANDROID POR BLUETOOTH .....	1428-1448
Mario Alberto Hernández Alves, Leonardo Sánchez, José A. Reyes Ortiz DISEÑO Y ANÁLISIS DE LA  DE UN MOTOR DE CC MEDIANTE LA SELECCIÓN ÓPTIMA DE PARÁMETROS. 1449-1462	
Jesús Alejandro Alvarez Tostado Uribe, Irma Martínez Carrillo, Carlos Juárez Toledo EMULACIÓN EN FPGA DE TÉCNICA PARA CORRECCIÓN DEL DESEQUILIBRIO I/Q APLICADO EN UN MODULADOR DIGITAL 256-QAM .....	1463-1482
Sergio Alberto Juárez Cazares, Aldo Bonilla Rodríguez, José Cruz Núñez Pérez GUÍAS DE DISEÑO WEB PARA FACILITAR EL ACCESO A LA INFORMACIÓN DESDE TELÉFONOS INTELIGENTES .....	1483-1505
Beatriz A. González Beltrán, Araceli Granados García FUSIÓN MORFOLÓGICA DE IMÁGENES IR Y VISUALES UTILIZANDO EL MODELO LIP .....	1506-1528
Oscar Ricardo Delfín Santiesteban, Iván Ramón Teró Villalobos INTERCOMUNICADOR ENLAZADO A RED DE TELEFONÍA CELULAR .....	1529-1549
Joel Fernando Acevedo Ruiz, Aldrin Barreto Flores, Verónica Edith Bautista López, Salvador Eugenio Ayala Raggi IMPLEMENTACIÓN DE UN SISTEMA DE ADMINISTRACIÓN Y CONTROL PARA UNA MICRO-RED DE CD UTILIZANDO PLATAFORMAS DE NATIONAL INSTRUMENTS .....	1550-1569
Juan José Martínez Nolasco, José Alfredo Padilla Medina, Elías José Juan Rodríguez Segura, Agustín Sancén Plaza CONTROL DEL FLUJO DE POTENCIA HACIA LA RED ELÉCTRICA DE UN SISTEMA DE GENERACIÓN ELÉCTICA EMPLEANDO UN GENERADOR DE INDUCCIÓN DE DOBLE ALIMENTACIÓN .....	1570-1590
Pedro Hernández Tenorio, Jaime José Rodríguez Rivas, Oscar Carranza Castillo, Rubén Ortega González ROBOT MÓVIL (3,0) UNA EVALUACIÓN DE RENDIMIENTO .....	1591-1611
Saul Enrique Benítez-García, Jorge Luis De-La-Cruz-Osorio, Miguel Gabriel Villarreal-Cervantes ONLINE PARAMETRIC IDENTIFICATION OF MASS-SPRING-DAMPER MECHANICAL SYSTEMS USING ACCELERATION MEASUREMENTS .....	1612-1625
Francisco Beltrán Carbajal, Gerardo Silva Navarro, Luis Gerardo Trujillo Franco SISTEMAS PARA LA EXTRACCIÓN DE FRASES CLAVE EN DOCUMENTOS CIENTÍFICOS .....	1626-1642
Gerardo Flores Petlalcalco, Mireya Tovar Vidal, Hilda Castillo Zacatelco, José A. Reyes-Ortiz MODELADO Y CONTROL DEL GIROSCOPIO ECP-750 .....	1643-1660
José Manuel Reyes Rodríguez, Fernando Reyes Cortés, J. Eligio Moisés Gutiérrez Arias CONTROL DIFUSO PARA UN CONVERTIDOR CD-CD APLICADO A SISTEMAS FOTOVOLTAICOS EN LOS MODOS MPPT Y CV .....	1661-1680
Julio Cesar Peña Aguirre, Agustín Ramírez Agundis, Elías J. J. Rodríguez Segura, Juan José Martínez Nolasco CONDITIONING AND SIGNAL AMPLIFICATION STAGES FOR A SMART GAS MICROSENSOR MEMS .....	1681-1698
J. L. González Vidal, M. A. Reyes Barranca, E. N. Vázquez Acosta TÉCNICA DE CONMUTACIÓN SUAVE PARA UN CONVERTIDOR REDUCTOR-ELEVADOR DOBLE CON APLICACIONES EN ILUMINACIÓN .....	1699-1718
Pablo Israel Guzmán Tafoya, Nimrod Vázquez Nava, René Osorio Sánchez	

REVISIÓN DE MÉTODOS PARA LA ESTIMACIÓN DE LOS ESTADOS DE CARGA Y SALUD DE UNA BATERÍA	1719-1736
Aina Araceli Contreras Sillero, Nimrod Vázquez Nava, Claudia Verónica Hernández Gutiérrez, Jeziel Vázquez Nava, Joaquín Vaquero López	
DESIGN, CONSTRUCTION AND SIMULATION OF A UNIFORM MAGNETIC FIELD GENERATOR WITH STEEL NUCLEUS TO DEFLECT COSMIC RAYS	1737-1756
Karla Natalia Herrera Guzmán, Raúl Alejandro Gutiérrez Sánchez, Jorge Luis Arceo Miquel, Julián Félix	
DEVELOPMENT OF A WIRELESS SIGNAL ACQUISITION SYSTEM FROM SENSORS FOR COMFORT AND ENERGY QUALITY	1757-1774
Israel Zamudio Ramírez, Arturo Yosimar Jaen Cuellar, Roque Alfredo Osornio Ríos	
BLOOD PRESSURE MEASUREMENT SYSTEM BASED ON OSCILLOMETRIC METHOD	1775-1794
Jessica Bolaños Olivera, Roque A. Osornio Ríos, Rosalía Reynoso Camacho	
IMPLEMENTACIÓN DE UN DETECTOR DE CAÍDAS PARA SU APLICACIÓN EN PACIENTES HOSPITALIZADOS Y PERSONAS DE LA TERCERA EDAD	1795-1808
José Luis Vázquez Avila, Walter Ariel Silva Martínez, Rafael Sánchez Lara, Casandra Sánchez Galván	
IDENTIFICACIÓN DE LOS FACTORES ADVERSOS QUE INFLUYEN EN LOS JÓVENES EGRESADOS PARA INCORPORARSE AL CAMPO LABORAL	1809-1828
Luis Alberto Morales Rosales, Mariana Lobato Báez, Ignacio Algreto Badillo, Héctor Rodríguez Rangel	
ELEMENTOS DE LOS PARQUES EÓLICOS QUE DEBEN SER CONTROLADOS PARA SU INTERCONEXIÓN CON REDES ELÉCTRICAS	1829-1845
Jorge Eduardo Hernández Miranda, Irvin López García, Eduardo Campero Littlewood, Francisco Beltrán Carbajal, Víctor Manuel Jiménez Mondragón	
CONVERTIDOR BIDIRECCIONAL MULTIFASE PARA APLICACIONES DE MICRO REDES DE CD	1846-1865
Jorge Rubén Morfín Orozco, Heriberto Rodríguez Estrada, Elías Rodríguez Segura	
VOLTMETRO BLUETOOTH Y DESPLIEGUE EN SMARTPHONE	1866-1888
Fernando Reyes Avilés, Carlos Avilés Cruz	
SELF-ORGANIZING MOBILE ROBOTS BASED ON MULTI-AGENT COORDINATION TECHNIQUES IMPLEMENTED WITH AERIAL VISION AND COMMUNICATION GATEWAY BETWEEN WIFI AND RF	1889-1905
Cynthia Daniela Briones Valencia, Zandor Alfredo Machaen Terriquez, Luis Martin del Castillo, Gustavo Alejandro Torres Blanco	
PREDICCIÓN DE POTENCIA FOTOVOLTAICA MEDIANTE REDES NEURONALES WAVELET	1906-1922
José Daniel Ortiz López, Luis J. Ricalde Castellanos, Braulio J. Cruz Jiménez, Ricardo J. Peón Escalante	
APLICACIÓN MÓVIL PARA EL CÁLCULO DE RUTAS "LOBOBICI" EN CIUDAD UNIVERSITARIA BUAP BASADA EN BÚSQUEDAS	1923-1938
Eliuh Cuecuecha Hernández, José Javier Martínez Orozco, Daniel Méndez Lozada, Adán Zambrano Saucedo, Aldrín Barreto Flores, Verónica Edith Bautista López, Salvador Eugenio Ayala Raggi	

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## CONDITIONING AND SIGNAL AMPLIFICATION STAGES FOR A SMART GAS MICROSENSOR MEMS

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### Resumen

En este trabajo, el objetivo principal es el diseño de una etapa nueva de amplificación y acondicionamiento de señal utilizando opamps, la cual será utilizada con un microsensar de gas inteligente. Las dimensiones del diseño fueron calculadas en base al modelo de pequeña señal de los MOSFET. Las configuraciones del opamp se eligieron de acuerdo a los requerimientos del sensor. El sensor está hecho de una película delgada de ZnO, depositada sobre la capa superior de una micropilaca sobre un microscopio micromaqueado. Gracias a la integración de las etapas de acondicionamiento de señal dentro del diseño, se dice que es un sensor inteligente. Se respaldó la operación de la etapa de amplificación y de acondicionamiento de señal por medio de técnicas de análisis de estabilidad, tales como el método del lugar geométrico de raíces. Se realizaron simulaciones y graficaron diagramas de Bode del sistema.

## Abstract

In this work, the principal aim is the design of novel signal amplification and conditioning stages using opamps, for an intelligent gas microsensor. The design dimensions were computed based on a small signal model of a MOSFET. The necessary configurations for the opamp were chosen according to the requirements of the sensor, which means, that the input signals are taken from this one. The sensor is based on a ZnO thin film deposited on the top side of a micro hot plate located within a micromachined pit. Thanks to the integration of signal conditioning stages within the design, it is said that it is an intelligent sensor. The right operation of the amplification stage and signal conditioning is supported by means of techniques of analysis of stability like the roots locus method, and computed Bode diagrams and simulations have been developed.

Keywords: Gas sensors, MEMS, opamp, smart sensors.

## 1. Introduction

Today, MEMS microsensors and smart sensors have very important and multiple applications in industry, automotive sector, aeronautics, biomedicine, consumer staples, etc. The most important advantages about MEMS are: their size (they are small devices), their low power consumption, batch fabrication and very low costs. MEMS sensors make a rich design space of networked sensors viable [González, 2006], [Howe, 1996].

Intelligent microsensors have a sensing stage and a conditioning stage due to the fact that the sensing stage provides a very low current in the nanoampere range [González, 2006]. Such current is a nonlinear signal and, since it is extremely low, it is hard to be manipulated by any ordinary electronic circuitry. For this reason, it is necessary to add linearization and amplification stages within the same monolithic integrated circuit. With these stages, undesired effects in the integrated circuit can be eliminated, such as parasitic charges, interface problems, noise, among others. [Vázquez, 2008]

The signal provided by the intelligent microsensor can then be converted to digital mode and then it be manipulated by a digital system or a digital computer.

## 2. Methods

Consider a gas microsensor which provides a small and nonlinear current signal. That signal must be amplified and linearized. With this in mind, an opamp was designed using CMOS technology.

### Three-stage opamp

A three-stage opamp was proposed as is shown in figure 1, where the first stage, A1, is a differential amplifier. The later has an input labeled  $V_{di}$ . The second stage, A2, is the gain stage, which decreases the gain at high frequencies; and the last stage, X1, provides gain in current mode.

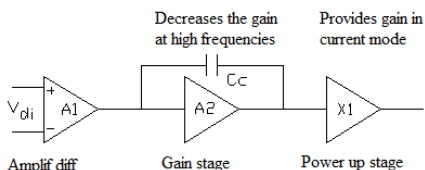


Figure 1 Three-stage opamp.

The diagram of the designed opamp is shown in figure 2. This opamp diagram was performed using Orcad® software. Subsequently, the opamp shall be explained in detail.

The Opamp design was developed according to AMIS 0.5 foundry technology and the layout was developed by using the L-Edit® software by Tanner-EDA. Values of  $L=2\lambda_D$ ,  $W=3\lambda_D$  and  $\lambda_D=1.5\mu\text{m}/2$  were proposed.

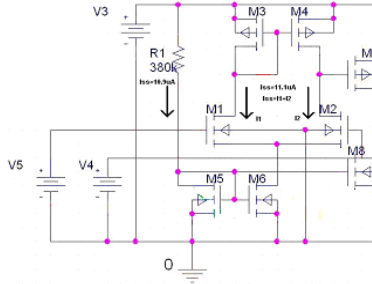


Figure 2 Opamp schematic circuit. M1 and M2 configure a differential pair, M3 and M4 form a current source load, M5, M6 configure a current mirror, and M7 and M8 configure a common source stage.

### Differential pair (inputs)

To better understand how opamp works, it was divided in several parts, the first one is the differential pair input.

The differential pair is formed by M<sub>1</sub> and M<sub>2</sub> n type transistors. It is well known that the current across the differential pair, comes from a current mirror (M<sub>3</sub> and M<sub>4</sub>, p type transistors). The dimensions of the transistors were calculated under the same conditions. That way, I<sub>SS</sub> is given by:

$$I_{SS} = \frac{K P_n}{2} \frac{W_{1,2}}{L_{1,2}} \mu_{n,55.6} \epsilon_{THN} \quad (1)$$

From (1)  $W_1=W_2=15.61 \mu\text{m}$  and  $L_1=L_2=15.75 \mu\text{m}$  and the current  $I_{SS}=10.09 \mu\text{A}$  were calculated, this current flows across M<sub>1</sub> and M<sub>2</sub>. For frequency compensation, these dimensions may be increased, even when the voltage applied affects too much adversely the current value which should be a constant value. [Vázquez, 2008], [Tsiviois, 1999], [Baker, 1997], [Gray, 2001].

The same design rules are now applied for p type transistors. The current source load was calculated to assure a  $I_{SS}=10.09\mu A$  current and a voltage of  $V_{GS3,4}=V_{THP}+0.3V=1.48V$ ,  $V_{DD}=5V$ ,  $V_{SS}=0V$ , then  $W_3$  can be calculated using (2):

$$I_{SS} = 0.09 \frac{\mu A}{L_3} \frac{K_{P,p} W_{3,4}}{2 L_3} V_{GS3,4}^2 V_{THN}^2 \quad (2)$$

$W_3=W_4=52.93\mu m$  and  $W_5=53.25\mu m$  and  $I_{SS}=10.15\mu A$  were calculated. This current parameter increases when the load potential of the current source load needs to decrease.

### Current mirror

To better understand how the differential amplifier stages work, it is necessary to understand how the current mirror works. This configuration is frequently used in circuit designing.

The current source was designed assuming that  $V_{DD}=5V$ ,  $V_{SS}=0V$ ,  $I_{SS}=10\mu A$   $V_{GS5,6}=0.85V$ , with these voltage and current values both saturations of  $M_1$  and  $M_2$  are assured. The value of R is calculated assuming that  $I_{D5} = I_{D6} = 10\mu A$ , if

$$I_D = \frac{V_{DD} - V_{GS}}{R} = \frac{K_{P,p} W}{2L_1} (V_{GS} - V_{THN})^2 \quad (3)$$

Solving for R

$$R = \frac{V_{DD} - V_{GS5,6}}{I_{SS}} \quad (4)$$

Therefore,  $M_5$  and  $M_6$  currents have the same values; both dimensions of  $M_5$  and  $M_6$  were calculated by using

$$I_{SS} = \frac{K_{P,p} W_{5,6}}{2 L_{5,6}} V_{GS5,6}^2 V_{THN}^2 \quad (5)$$

Although there is a small increase in the power consumption and the gain decreases, this will not affect the designed circuit.

Output impedance is denoted by:

$$r_o = \frac{f_c}{I_D} \cdot \frac{1}{\frac{1}{L_b}} \quad (6)$$

$L_b$  is calculated based on experimental data (0.06V<sup>-1</sup> typical), in this case

$$r_{o6} = \frac{1}{\frac{1}{L_{SS}}} \cdot \frac{1}{0.06V^{-1}} \cdot \frac{1}{11.23 \mu A} \cdot 63MEG \Omega \quad (7)$$

### Common source stage (output)

This stage is formed with transistors M<sub>7</sub> and M<sub>8</sub>. Transistor M<sub>8</sub> is biased as current source and the input of the amplification stage is connected to the gate of M<sub>7</sub>.

The current through M<sub>8</sub> and the current mirror (M<sub>5</sub> and M<sub>6</sub>) must be the same. Therefore, M<sub>8</sub>, M<sub>5</sub> and M<sub>6</sub> have the same dimensions W<sub>5</sub>=W<sub>6</sub>= W<sub>8</sub>=15.61 μm, L<sub>5</sub>=L<sub>6</sub>=L<sub>8</sub>=15.75 μm, whereas M<sub>7</sub> has the same dimensions than M<sub>8</sub>, therefore, the value of the current mirror and the differential pair is the same current.

Once the simulation is carried out, the transistor dimensions should be adjusted to fulfill the polarization requirements, signal conditioning, power consumption, stability and gain, among others [Vázquez, 2008], [Razavi, 2001], [Giurgiutiu, 2010], [Schilling, 1999].

### 3. Results

With the objective of determining the characteristics of the opamp, the circuit performance was simulated, 2.5V were applied to the non-inverting input (V5) with two voltage sweeps. The first sweep is from 0V to 5V and the second one from 2.47V to 2.53 with 0.001V steps in the non-inverting terminal (V4).

The diagram of opamp was simulated with Orcad® software, according to the parameters of V3.1, level 7 of AMIS 0.5 μm technology libraries, equations have a complexity degree of level 3. The results from simulations are shown in figure 3, where the I<sub>SS</sub> in M<sub>5</sub> is raised to 10.9 μA due to channel modulation effects (figure 3.a), and I<sub>SS</sub> in M<sub>6</sub> is raised to 11.1 μA (figure 3.b). On the other hand, voltage V<sub>GS</sub>

in  $M_5$  is 858mV (figure 3.c). From figure 3.d it is shown that the equation  $V_{GSS} \geq 0.3V + V_{THN}$  is satisfied which means that the transistors are in saturation. [Vázquez, 2008]

Gain

Gain is expressed by the next equation:

$$A_{OL} = \left( \frac{g_{m1}}{g_{m2}} \right) \left( \frac{r_{o1}}{r_{o2}} \right) \left( \frac{r_{o3}}{r_{o4}} \right) \left( \frac{r_{o5}}{r_{o6}} \right) \quad (8)$$

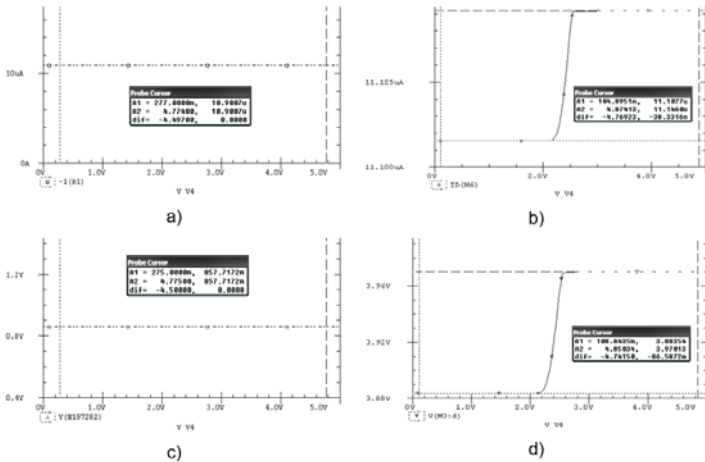


Figure 3 Simulation plots of schematic of figure 2.

From figure 4, it can be determined that the gain is given by

$$|A_{OL}| = \frac{Output}{Input} = \frac{2.93V}{6815 \mu A} = 4.305 \quad (9)$$

Gain is modified due to body effect. Gain results in the  $\frac{V_{GS}}{I_{SS}}$  variation and, in consequence, the variation of Eq. 8. The output current of the second stage will be the same current of the design, this means  $I_{SS} = 10.9 \mu A$ .



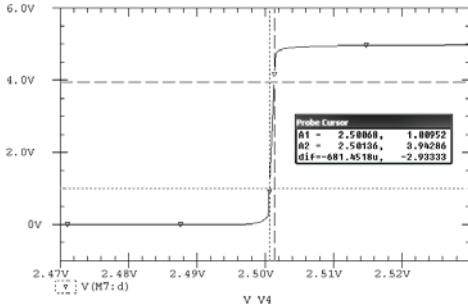


Figure 4 Opamp response due two voltage sweeps applied.

### Small signal analysis

In a two-stage amplifier, figure 5, and considering high impedance nodes, which determine the dominant poles, the output resistance  $R_1$  of the opamp is connected to ground, is given by:

$$R_1 = \left[ \frac{r_{o2}}{1 + \beta_2} \right] \parallel r_{o4} \quad (10)$$

Where both  $r_{o2}$  and  $r_{o4}$  are the output impedances of  $M_2$  and  $M_4$  respectively.

Capacitance  $C_1$ , can be calculated using:

$$C_{TOT} = C_L \parallel C_{dg7} \parallel C_{db4} \parallel C_{gd4} \parallel C_{db2} \parallel C_{gd2} \quad (11)$$

Where  $C_{TOT}$  is the total capacitance of the circuit, the load capacitance  $C_L$  is  $C_{dg7} + C_{gs7}$ , which are drain-gate and gate-source capacitances of  $M_7$ ,  $C_{db4}$  and  $C_{gd4}$  are drain-bulk and gate-drain capacitances of  $M_4$ ,  $C_{db2}$  and  $C_{gd2}$  are drain-bulk and gate-drain capacitances of  $M_2$ . Since  $C_{dg7}$  is connected between the input and the output of the amplifier, the Miller theorem can be applied to divide the capacitance in two parts. The first capacitance is connected to the input and the second one to the output of the amplification stage. Miller capacitances are supposed to be

connected to the gate and to the physical ground and between the drain and the physical ground; then, the load capacitance is now:

$$C_L = C_{gs7} + C_{MI} \tag{12}$$

Where  $C_{MI}$  is known as Miller input capacitance,  $C_{MI}$  is denoted by:

$$C_{MI} = C_{gd7} (1 + |A_2|) \tag{13}$$

and  $C_{MO}$ , the output miller capacitance, is denoted by

$$C_{MO} = C_{gd8} (1 + |A_2|) \tag{14}$$

On the other hand, the drain node of  $M_7$  is characterized by  $R_2$  and  $C_2$ , where  $R_2 = R_1$ , because the current of polarization is the same.

$C_2$  is given by:

$$C_2 = C_{gd7} + C_1 \frac{1}{|A_2|} + C_{db7} + C_{db8} + C_{gd8} \tag{15}$$

Finally, the calculated values are  $R_1 = R_2 = 1502k\Omega$ ,  $C_1 = 1.14pF$  and  $C_2 = 1.84fF$ . [Vázquez, 2008], [Giurgiutiu, 2003].

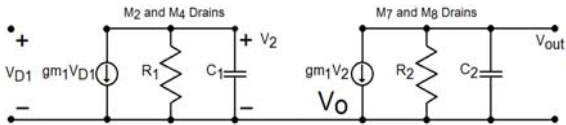


Figure 5 Small signal model of a two stages amplifier.

### Frequency response analysis

The closed-loop gain of the opamp is described in terms of

$$A_{CL} = \frac{A_{OL}}{1 + \beta A_{OL}} \quad (16)$$

where  $A_{OL}$  is the open loop gain of the opamp.

The amplifier reaches stability when:

$$|A_{OL} \beta| = 1 \quad \text{and} \quad \angle A_{OL} \beta = 180^\circ \quad (17)$$

Where  $\beta$  represents the amount of output signal that could be feedback and subtracted to the input of the amplifier; the highest possible value of  $\beta$  with amplification is given when  $\beta=1$  and this condition is achieved in the voltage follower configuration.

Figure 6 shows the Bode plots resulting from the simulations. These were performed using the Orcad® software, applying an input signal of 0.01Hz up to 10GHz, with 10-decade steps. In figure 6a, the system shows a unit gain (0dB), which corresponds to a phase angle of  $45^\circ$ , whereas figure 6b shows that the gain is -25.997dB, which means that the system does not require external compensation [Vázquez, 2008], [Razavi, 2001], [Giurgiutiu, 2010], [Schilling, 1999].

Opamp characterization

One quality of the opamp is to reject a common signal (CMRR) applied to its two inputs and it is represented by the gain in common mode given by:

$$CMRR = 20 \log \left| \frac{A_d}{A_c} \right| = 20 \log \left| g_{m1} \frac{R_{D1}}{R_{D2}} \left( \frac{R_{D1}}{R_{D2}} + 1 \right) \right| - 20 \log |g_{m4} r_{o6}| \quad (18)$$

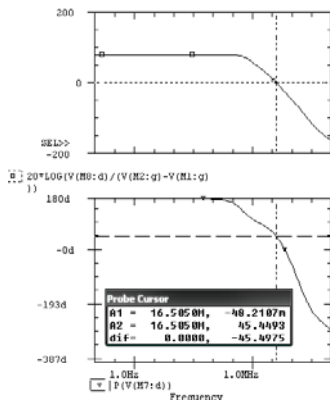
In figure 7 it can be noticed that  $CMRR=-42.92\text{dB}$ , which is a convenient value for a good performance of the amplifier. On the other hand, the power supply rejection ratio (PSRR) is used to describe the amount of noise that a voltage power supply of a particular device can reject.

$$PSRR = A_{OL} \left( \frac{v_{out}}{v_{sin}} \right) \quad (19)$$

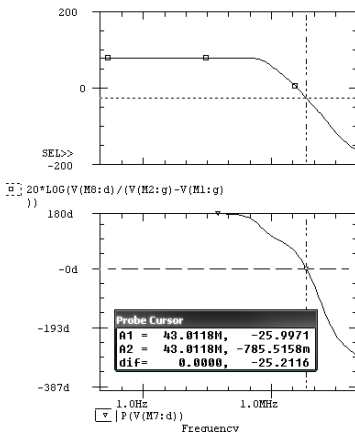
Where  $A_{OL}$  is the open-loop gain,  $v_{out}$  is output voltage and  $v_{sin}$  is input sinusoidal voltage; for this opamp PSRR = -3.704dB. Figure 8 shows the maximum cut frequency, where a  $f_{max} = 195$  KHz can be noticed. [Vázquez, 2008].

#### Gas sensor-opamp connection

It is well known that electrical properties of semiconductors have a tight dependence on temperature. In the case of semiconductor oxides, a ZnO thin film must reach temperatures close to 300°C so the right adsorption and reduction processes can be correctly carried out in presence of oxidizing or reducing species. The main characteristic of a ZnO thin film is that the variation of its resistance is not a linear in presence of a reducing species such as CO. For this reason, the most of gas sensors are based on thin films of semiconductor oxides, this process is explained in detail in [González, 2005, 2006, 2013].



a) Gain margin,



b) Phase margin.

Figure 6 Bode plots a) Gain margin, b) Phase margin.

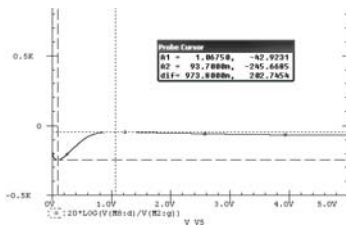


Figure 7 Common mode gain (CMRR) for an input signal applied (0 through 5V, with 0.0001v steps).

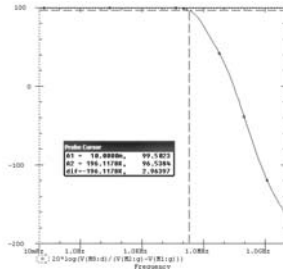


Figure 8 PSRR simulation.

In figure 9, the behavior of a gas sensor can be observed. The gas sensor measurements were compared to simulations that were carried out using Matlab® and Orcad® softwares. The use of a 100MΩ resistance in series (voltage divider) with the gas sensor, allowed getting voltage values for different CO concentrations. Due to sensor resistance variation, it cannot be measured directly. For this reason, an opamp in voltage follower configuration is connected to the voltage divisor output; this allows the interaction between the gas sensor and the load. In this case, the load is a variable gain amplifier (VGA).

Since the output in voltage mode of a voltage divisor has a logarithmic behavior, an output in a proportional voltage mode of CO concentration is desired. The VGA provides a linear variation of output voltage of the signal conditioning stage, with respect to a CO concentration variation. After analyzing the slope of the logarithmic plot, there are four regions where such variation of the plot is minimum. Therefore, the VGA has four possible changes in its gain (although there might be fifteen changes). Each of the four regions already mentioned have different slopes that must be interpreted. VGA lets every region to have the same slope; nevertheless, the slope increases or decreases the voltage value in each region, which means that it moves the whole region upwards or downwards. That is why compensation voltages are required. Compensation voltages are different in each region and they

depend on the gain. Voltages are added or subtracted to a whole region depending on whether the signal is amplified or attenuated, respectively. [Vásquez, 2008]

The current follower circuit is connected to the VGA output with the purpose of avoiding any interaction with the load. Figure 10 shows the schematic circuit. It was designed with connections for external resistances, because external resistances can modify the gain. First and third terminals are designed for power supply connection. The second terminal is designed for connection of the  $100M\Omega$  resistance,  $V_{div}$  is the output voltage of  $A_{s1}$ ; an input resistance  $R_1$  is connected to  $V_{div}$  and  $R_1$  terminals;  $V_c$  is the voltage that compensates the gain change of  $A_{gv}$ ;  $Cv_{1,2,3,4}$  are control signals which determine feedback resistance. Feedback resistances  $R_f$  are connected between  $R_{f1,2,3,4}$  and  $V_{fb}$ . The output signal of  $A_{gv}$  is connected to the non-inverting output of the current follower  $A_{s2}$ .  $A_{s2}$  avoids the load to drain current to  $A_{gv}$ , and finally  $V_{out}$  is the output voltage of the circuit. [Vásquez, 2008]

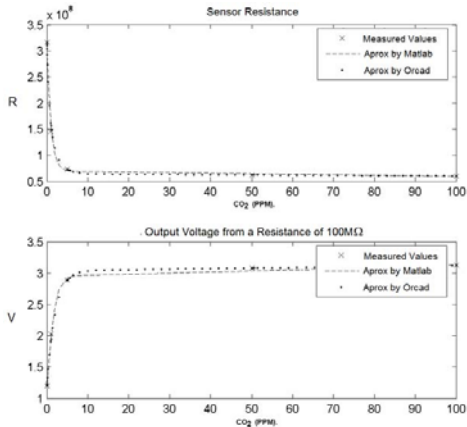


Figure 9 Variation of sensor resistance and voltage divider output potential for several  $CO_2$  concentrations.

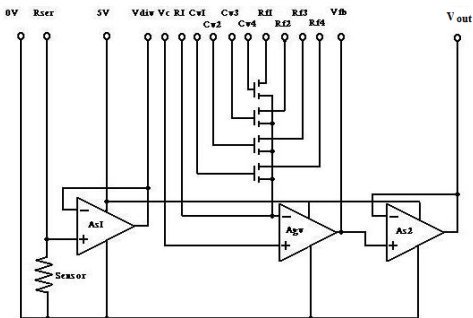


Figure 10 Schematic circuit developed.

#### 4. Discussion

The signal conditioning stage is very important, because sensor signal linearization is needed. The sensor's linear signal is taken to a standard range for right measurements. Signal conditioning stages must have a right approximation of the sensor's behavior. The approximations were developed by Matlab® using recursive gradient method. However, Orcad® allows designing more accurate functions for the electrical behavior of the device, because resistive, capacitive and inductive elements are used. Nevertheless, the functions developed in Matlab® had problems when they were translated to Orcad®.

On the other hand, the use of PMOS instead of NMOS makes all the transistors not to work in a saturation mode, and it was observed that their behavior was unstable. The use of a logarithmic conditioning stage does not work because the constants defined in this stage are different from the sensor's response parameters; therefore, they do not eliminate each other. Finally, using a resistance of  $100M\Omega$  in series with the gas sensor allows obtaining voltage values for different CO concentrations. Since the sensor resistance variation cannot be measured



directly, an opamp in current follower configuration is connected to the voltage divisor output, and generating the possibility of interaction between the gas sensor and the load. In this case, the load is a VGA. The realization of this on-chip device will be developed.

## 5. Conclusions

A three-stage opamp was designed, such stages are three opamps called A1, A2 and X1; since this circuit will have a special application, a lot of values were computed.

In realizing of the opamp design, it was divided in a differential pair (formed by  $M_1$  and  $M_2$  transistors), current load source (formed by  $M_3$  and  $M_4$  transistors), current mirror (formed by  $M_5$  and  $M_6$  transistors) and common source stage (formed by  $M_7$  and  $M_8$  transistors). Drain currents  $I_D$  and transistor dimensions as  $W$  and  $L$  were calculated. Opamp design was developed according to 0.5 $\mu\text{m}$  AMIS technology and the layout was developed by using L-Edit software by Tanner EDA. Simulations were developed using Matlab® and Orcad® softwares. Several characteristics of the opamp were analyzed, such as gain, small signal analysis, frequency response analysis; in addition, CMRR and PSRR were calculated.

Opamp design and calculations were based on basis of semiconductors, electrical physics, magnetism concepts, modeling and transistors performance. In addition, frequency stability was applied. Computational techniques gave us a very reliable approximation of the performance and behavior of the opamp. The designed Opamp was developed according to a particular gas sensor whose surface resistance varies two orders of magnitude.

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